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## AUTHOR'S RELEVANT PUBLICATIONS

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### **Publications in Referred Journals:**

1. **V Nallasamy**, S K Datta, SUM Reddy and P K Jain, "Efficiency Enhancement of an S-band Magnetically Insulated Line Oscillator," *International Journal of Microwave and Optical Technology (IJMOT)*, vol.11, No.5, pp. 324-331, Sept 2016
2. **V Nallasamy**, "Sources for high Power Microwaves", *Defence Science Spectrum*, pp. 225-234, February 2012.
3. **V Nallasamy**, C Narasimhamurthy, B Geetha, Sanjay Kumar Gupta, Subrata Kumar Datta, SUM Reddy and P K Jain, "Electromagnetic Simulation and Experimental Characterization of RF Interaction Structure of an S-band Magnetically Insulated Line Oscillator," *Journal of Electromagnetic Waves and Applications(JEMWA)*, - accepted for publication .
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1. **V Nallasamy**, S K Datta, SUM Reddy and P K Jain, "Design and Simulation of Magnetically Insulated Line Oscillator," Proceedings of National conference on Vacuum Electronic Devices and Applications, Sep .21-24,2012.
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## Efficiency Enhancement of an S-band Magnetically Insulated Line Oscillator

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**Abstract-** An improved Magnetically Insulated Line Oscillator (MILO) operating in S-band was designed using analytical formulation and was simulated using 3D-electromagnetic particle-in-cell (PIC) code. The Dispersion characteristics of the RF interaction structure was analytically obtained using equivalent circuit approach, and subsequently the performance was optimized using particle-in-cell analysis for operation around  $\pi$ -mode resonant frequency of 3.3 GHz. The region of operation of this MILO was obtained under para-potential flow using Hull-cut off and Buneman-Hartree conditions. The design was optimized for improving the efficiency by suitable tailoring of the lengths of cathode, beam dump, extractor cavity gap and the position of stub at the output of the device. The design was performed for 500 kV, 47.5 kA and simulated output power of around 6 GW in TM<sub>01</sub> mode could be achieved at the frequency of 3.1 GHz with the power conversion efficiency of around 25%.

**Index Terms-** Electromagnetic PIC simulation, Dispersion relation, high power microwave, Magnetically Insulated Line Oscillator (MILO).

### I. INTRODUCTION

MILO is a GW-class cylindrical crossed-field oscillator invented by Lemke and Clark [1] in 1987, and became popular for its potential as a high-power microwave (HPM) source for military applications (Fig.1). It has a unique magnetic self-insulating property that enables the tube to handle extremely large input power (tens to hundreds of GW) at a modest applied voltage (several hundred kilovolts). It does not require any externally applied DC magnetic field, which allows the conceptualization of a compact and light weight HPM source. At high voltages,

electrons are emitted from the cathode but the current carried by the body (anode) creates a sufficiently strong magnetic field such that these electrons cannot cross the interaction gap. The electrons drift axially in the crossed electric and self-generated magnetic fields. The slow-wave structure (SWS) facilitates the interaction between the axially drifting electrons (the region adjacent to the cathode) and the axially directed slow electromagnetic wave to generate microwaves. However, it suffers from the fundamental limitation of low RF conversion efficiency. This is due to the utilization of maximum load current for generating the self-magnetic field [2–4]. The first ever MILO developed by Lemke *et al.*, [4] that has output power of 2.1GW power at L-band with an efficiency of 10.3%. The highest efficiency in an experimental MILO has been achieved so far is ~11%.

Marder simulated the behavior of MILO with 47 kA, 195 kV electron beam to get ~2GW at L-band with an efficiency of ~11% [3]. Kim *et al.*, experimentally studied an axial mode competition in a GW MILO with a pulse duration of 130 ns and verified through a PIC code [6]. Cousin *et al.*, developed a compact MILO based on the U.S. Air Force geometry that was operated in  $3\pi/4$  mode with a beam voltage of 600 kV [7]. In 2009, Li *et al.*, tested an improved tapered MILO for 2GW of peak RF power in TM<sub>01</sub> mode at 2.63 GHz with a conversion efficiency of ~11% [8]. In 1998, Eastwood *et al.*, developed a tapered MILO with a simulation efficiency of ~30% [9]. Qin *et al.*, simulated an S-band higher order mode depressed MILO based on an existing L-band



ladder cathode MILO at 1.2GHz using an electron beam of 830 kV interacting with a transverse electromagnetic (TEM) mode to obtain an RF power of ~6GW at 2.48 GHz [10].

In this article, the design and simulation of an S-band MILO is presented to improve its overall efficiency by reducing the total length and proper impedance matching at the output by using stubs. The rest of the article is organized as follows: the analytical design methodology and the dispersion of MILO are presented in Section II. The 3D modeling and PIC simulation of the improved MILO are narrated in Section III. The technique of efficiency enhancement is briefed in Section IV and the conclusion is drawn in Section V.

## II. DESIGN METHODOLOGY

We have considered a MILO with the slow-wave structure comprising periodically spaced cavities formed by placing apertures in a smooth waveguide, as shown in Fig. 2. The slow-wave structure supports number of slow-wave modes. Suitable phase synchronism between any one of these electromagnetic modes and the drifting electrons (with velocity  $v_d = E_o / B_o$ , where  $E_o$  and  $B_o$  are the electric field in radial direction and magnetic field in azimuthal direction, respectively) results in efficient conversion of beam energy to RF energy.

The resonant frequency,  $\omega_o$  of an individual SWS cavity of the MILO can be expressed in terms of the circuit parameters following equivalent circuit approach as [11]:

$$\omega_o = \left( \frac{\mu_o z d}{4\pi r_o} \left[ 2\epsilon_o r_i \ln\left(\frac{z/2+w}{z/2}\right) + \frac{2\pi\epsilon_o}{3zd} (r_o^3 + 2r_i^3 - 3r_o r_i^2) \right] \right)^{-1/2} \quad (1)$$

where,  $\mu_o$  is the permeability of free-space;  $z$  is the distance between the SWS apertures;  $r_o$  and

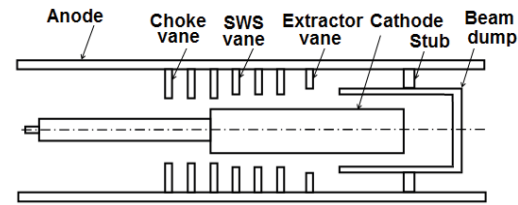


Fig.1. Schematic of Magnetically Insulated Line Oscillator.

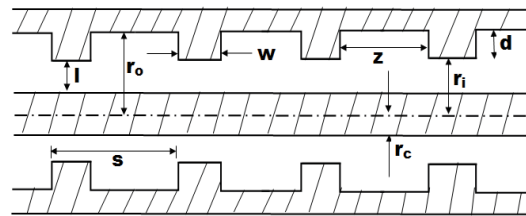


Fig.2. Schematic of coaxial disk loaded SWS.

$r_i$  are the outer and inner radii of the SWS vane;  $d = r_o - r_i$  is the vane height;  $w$  is the thickness of the SWS vane;  $r_c$  is the cathode radius;  $s$  is the circuit periodicity; and  $l = r_i - r_c$  is the free space gap between anode to cathode. For a slow-wave structure comprised of  $N$  number of cavities, the resonance condition would necessitate the following condition to satisfy:

$$2N\phi = 2k\pi \quad (2)$$

where,  $N$  is the number of SWS cavities;  $k$  is an integer and  $\phi$  is the phase difference between the adjacent cavities. The resonant frequency of the coupled cavity stack,  $\omega_{ok}$  can be now given as [11]:

$$\omega_{ok} = \omega_o \left( 1 + \frac{\frac{2\pi\epsilon_o w}{\ln(r_i/r_c)} + 8\epsilon_o \left[ z + \left( r_i - \frac{2l}{\pi} \right) \ln\left( 1 + \frac{\pi z}{2l} \right) \right]}{2 \left[ 2\epsilon_o r_i \ln\left( 1 + \frac{2w}{z} \right) + \frac{2\pi\epsilon_o}{3zd} (r_o^3 + 2r_i^3 - 3r_o r_i^2) \right]} \right)^{-1/2} \left( \frac{1}{1 - \cos\phi} \right) \quad (3)$$

When cathode current becomes higher than the critical current, the self-magnetic field generated confines the electrons and it does not reach up to the anode. The electrons derive equipotential surfaces and move perpendicular to the crossed



electric and magnetic fields. The minimum current or critical current  $I_{cr}$  required to insulate the beam is defined as [12]

$$I_{cr} = I_0 \sqrt{\gamma_o^2 - 1} / \ln(r_i / r_c) = \frac{4\pi m_0 c^3 \epsilon_o \sqrt{\gamma_o^2 - 1}}{e \ln(r_i / r_c)} \quad (4)$$

where,  $r_c$  and  $r_i$  are the cathode and anode radii, respectively;  $I_0$  is the starting current for oscillation,  $e$  is the electron charge and  $m_0$  is the electron mass at rest;  $\gamma_o = (1 - \beta^2)^{-1/2}$  is the relativistic mass factor with  $\beta = v_d/c$  as the normalized electronic drift velocity with respect to the velocity of electromagnetic wave in free-space as evaluated at the anode. As the insulated electron flow fills the anode-to-cathode gap (A-K-gap), the total anode current or para-potential current,  $I_p$  becomes [12]

$$I_p = \frac{I_0 \gamma_o \ln(\gamma_o + \sqrt{\gamma_o^2 - 1})}{2 \ln(r_i / r_c)} \quad (5)$$

Under the condition of Diocotron instability [13], few of the electrons of the beam reach the anode and few others remain at the magnetic cutoff, while the other electrons migrate towards the anode in bunch form (usually called as spokes). The mode of oscillation of MILO is established when electron drift velocity is slightly greater than the phase velocity of the RF wave. The condition of synchronism is given as [14]:

$$v_d = \frac{E_0}{B_0} = \frac{V_0}{2 \ln(r_i / r_c)} \left( \frac{2\pi r}{\mu_0 I_t} \right) = \frac{2\pi \epsilon_o c^2}{\ln(r_i / r_c)} \left( \frac{V_0}{I_t} \right) \cong 0.3c \quad (6)$$

where,  $v_d$  is the electron drift velocity;  $\epsilon_o$  is the permittivity of free-space;  $I_t$  is the total anode current. The RF phase velocity,  $v_\phi$  at which electronic interaction could take place can be now expressed under the condition of synchronism,  $v_\phi \approx v_d$  as [14]:

$$v_\phi = \frac{s}{2dc} \cong 0.3c = \frac{\omega}{\beta_0} = \frac{2\pi f}{(\pi/s)} = 2sf \quad (7)$$

where,  $\omega$  is the angular frequency,  $s$  is the periodicity of the slow-wave structure (SWS),  $d$  is the vane height,  $f$  is the operating frequency, and  $\beta_0$  is the axial propagation constant. In order to complete the design, it would be now required to arrive at the length of the load, the length of the cathode and the efficiency of the device. These parameters are arrived at from the consideration of Hull cut-off and Buneman-Hartree conditions. The cathode current  $I_c$  under Hull cut-off criteria is defined as [14]

$$I_c = \frac{8500}{\ln(r_i / r_c)} \left[ \frac{eV_H}{m_0 c^2} \left( 2 + \frac{eV_H}{m_0 c^2} \right) \right]^{\frac{1}{2}} \quad (\text{Hull cut-off}) \quad (8)$$

Here,  $V_H$  is the Hull cut-off voltage;  $e$  and  $m_0$  are the charge and mass of electrons at rest, respectively. The relation between the cathode current,  $I_c$  and the Buneman-Hartree voltage,  $V_{BH}$  is given by [14]

$$I_c = \frac{8500}{\beta_0 \ln(r_i / r_c)} \left[ \frac{eV_{BH}}{m_0 c^2} (1 - \sqrt{1 - \beta^2}) \right] \quad (9)$$

For a given operating voltage, when the minimum load length is decided at the condition of charging current reaching the value of critical current,  $I_{cr}$ . Under such condition, the minimum length of load,  $L_{Cmin}$  is defined by [4],

$$L_{Cmin} = 2r_c \ln \left( \frac{r_i}{r_c} \right) \frac{\sqrt{\gamma^2 - 1}}{[G(\gamma_0)]^2} \quad (10)$$

where,  $G(\gamma_0) \approx 2(\gamma_0^{1/2} - 0.847)$ . The length of the cathode,  $L_{SE}$  is arrived from the perveance of the device  $\mu = I_c/V_o^{3/2}$ , given as [15]:

$$L_{SE} = 6.82 \times 10^4 \mu r_i (\ln(r_i / r_c))^2 \quad (11)$$

where,  $\mu$  is the diode perveance that depends on geometrical parameters,  $I_c$  is the cathode current and  $V_o$  is the cathode voltage. The corresponding maximum efficiency,  $\eta_{max}$  of the MILO relative to the input beam power is given by [4]:

$$\eta_{max} = \frac{P_{max}}{V_o I_p} = 0.32 \left( \frac{I_{s,max}}{I_p} \right) = 0.32 \left[ 1 - \left( \frac{I_{cr}}{I_p} \right) \right] \quad (12)$$

where,  $P_{max} = 0.32 * I_{s,max} * V_o$  and  $I_{s,max} = I_p - I_{cr}$ , is the maximum total dc spoke current,  $V_o$  is dc A-K gap voltage, and  $P_{max}$  is the corresponding output power of the MILO. The maximum power conversion efficiency is possible to be obtained for the condition of transit angle corresponding to the gap approaching  $\pi$  which is accounted for with the numerical value of 0.32 as given in the equation (12). However, both simulations and experiments for a load-limited MILO have shown efficiencies quite close to those predicted by (12). The region of operation of the proposed device with  $r_c = 25$  mm,  $r_i = 40$  mm,  $s = 13$  mm, and  $2d = 42.8$  mm as obtained from the analysis is shown in Fig. 3. The dispersion characteristics of the four cavity slow wave structure operating in  $\pi$ -mode at the frequency of 3.3 GHz is shown in Fig. 4 as computed using the equivalent circuit analysis. The device operates at a constant voltage within the regime  $V_{BH} < V < V_H$  with the electron beam intensity limited by self-generated magnetic field. The Buneman-Hartree condition does not become prevalent due to the corresponding plot remains below the parapotential current.

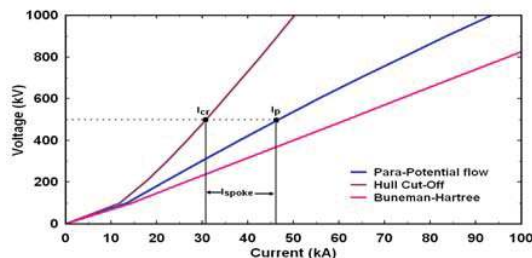


Fig. 3. Region of operation of the MILO for  $r_c = 25$  mm,  $r_i = 40$  mm,  $s = 13$  mm,  $2d = 42.8$  mm.

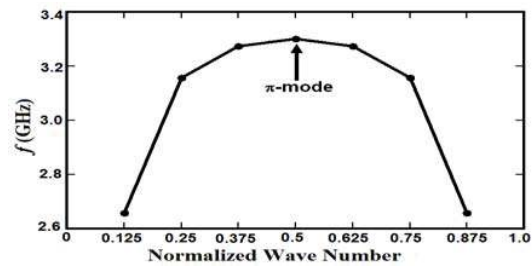


Fig. 4. Dispersion characteristics of the four cavity SWS.

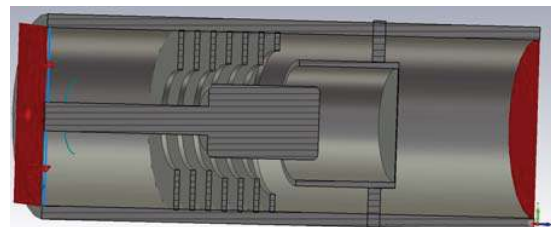


Fig. 5. 3D model of the proposed MILO in CST environment.

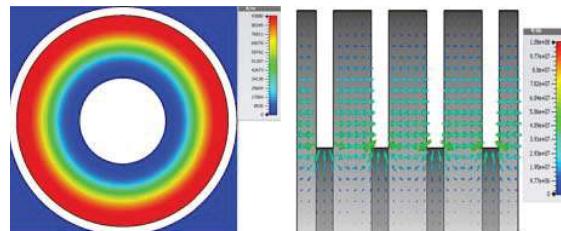


Fig. 6. (a)  $TM_{01}$  field pattern, and (b)  $\pi$ -mode in SWS of MILO.

### III. MODELING AND SIMULATION OF MILO

#### A. Beam-Absent Cold Simulation

In our design, the RF section comprises seven vanes: three choke vanes, three SWS vanes, and one extractor vane. The first three vanes (choke vanes) constitute the RF choke cavity that is operated at frequency less than the pi-mode frequency. The dimensions of the next three vanes (SWS vanes) decide the frequency of oscillation as the beam-wave interaction takes place in this region. The inner radius of the last vane (extractor vane) is kept larger than SWS vanes and it plays a vital role in extracting RF energy from the interaction region. The extractor vane and beam dump form the RF extracting



cavity. The 3-D modeling of the device was carried out using CST Studio with adaptive mesh refinement. A 3-D schematic of the MILO with short-length cathode is shown in Fig. 5. The design parameters used in the present model are shown in Table 1. All the vanes including choke, SWS, beam dump, cathode, anode, and stubs of MILO structure have been modeled using a perfect electric conductor (PEC) with background as vacuum. The MILO structure has been modeled and simulated in the linear co-ordinate system using hexahedral meshing. Both electric and magnetic fields satisfy the boundary conditions imposed by the walls of the RF circuit. The Eigen-mode analysis has been carried out for the desired  $TM_{01}$ -mode in the SWS (Fig. 6). The  $E$ -field in adjacent cavities are  $180^\circ$  out of phase which confirms the  $\pi$ -mode of operation at 3.3 GHz. The field distribution associated with  $\pi$ -mode produces the strongest coupling to the electron beam with high Q (quality factor) space-harmonics. To maximize the power output in our improved MILO, four short-circuited stubs are placed at 90 degrees apart that provide return path for electron beam. These are mechanically joined to the extractor and anode for impedance matching and also acting as a short circuit for dc but an open circuit for RF.

### B. Beam-present Hot Simulation

A few assumptions are used for the PIC simulation: the electric and magnetic fields are assumed to be confined to the space within the RF interaction circuit, dielectric loss is negligible, and the power loss at the metallic boundaries is also negligible. For the beam-present simulation, four discrete ports at  $90^\circ$  apart have been defined at the input port of the MILO for applying high voltage between the cathode and the anode. In the RF circuit of MILO, electrons have been considered as uniformly longitudinally distributed, and their evolution along the axial direction in the presence of RF noise has been monitored in time domain. A beam voltage of 500kV with the rise time of 1ns was applied between cathode and anode at the input port to facilitate generation of electron beam due to

explosive emission from the surface of a cylindrical velvet cathode.

Table 1: Optimized Design Dimensions of MILO

Parameters	Designed Parameters	Optimized Parameters
SWS vane radius ( $r_i$ )	40 mm	39 mm
Extractor vane radius ( $r_{ex}$ )	48 mm	49 mm
Cavity Period (s)	12.9 mm	13 mm
Beam dump inner radius	40 mm	39 mm
Beam Dump outer radius	44 mm	43 mm
Beam Dump length	164.4 mm	84.4 mm
Cathode projection inside Beam Dump	123.4 mm	7.4 mm
Length of cathode	200mm	80mm
Total length of MILO	373.8mm	289.8mm

Due to the self-generated magnetic field, electron beam remains insulated between the SWS vanes and cathode. The electron distribution was observed to be axis-symmetric in each transverse cross section in the  $yz$ -plane at  $t = 65.72$  ns as shown in Fig. 7. In order to observe the growth of the RF field, we set a number of electric field probes. The generation of RF power was monitored at the output port. The impedance discontinuity between the choke vanes and SWS vanes benefitted the MILO operation as the high impedance in the choke vane section resulted in lower E-field to avoid electrical breakdown and the low impedance in SWS vane section resulted in high spoke current. The higher spoke current due to more electrons at the interaction region enhanced the efficiency to  $\sim 25\%$  as compared to the similar conventional MILOs that offer efficiencies of  $\sim 15\%$  [16] and  $12\%$  [10]. The E-field amplitude at the output port was obtained as 80 kV/m (Fig. 8). The RF output of  $\sim 6$ GW was observed (Fig. 9) at 3.1GHz in  $TM_{01}$ -fundamental mode of operation with beam current of 50 kA and beam voltage of 500 kV (Figs. 10 and 11). The Fourier transform of E-field amplitude shows the desired frequency of operation as 3.1 GHz as shown in Fig 12. The magnetic field distribution at the output port (Fig. 13) clearly indicates that the improved design operates in fundamental mode. The microwave



frequency obtained from the simulation is 3.1 GHz against that of the cold  $\pi$ -mode frequency of 3.3 GHz. The shift in the simulated operating frequency is attributable to the beam loading effect. The energy distribution over the interaction length at  $t = 95$  ns is shown in Fig. 14.

#### IV. EFFICIENCY ENHANCEMENT

The enhancement of overall efficiency was obtained by reducing the inner radius of choke vane, SWS vane, Extractor vane and Beam dump by 1mm. In addition to the above the position of stubs on the beam dump played vital role in matching the impedance at the output of MILO in order to extract maximum RF power. A part of the cathode extended into the Beam dump was reduced from 164.4mm to 7.4mm for maintaining the sufficient load length required to generate the critical current for generating the required self-magnetic field and also the reduced cathode length helped in preventing off axis shift due to cantilever force and thus asymmetric emission of electron beam is prevented. In view of the above, the overall efficiency of the Improved MILO is enhanced to 25% for the voltage of 500kV and current of 47.5kA.

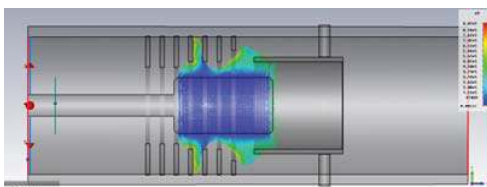


Fig. 7. Distribution of electrons at 65.72 ns

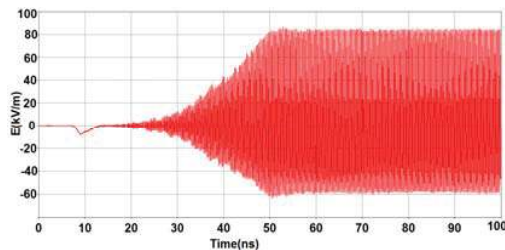


Fig. 8. Instantaneous E-field amplitude

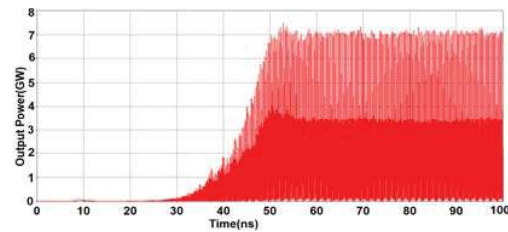


Fig. 9. Peak output power of improved MILO

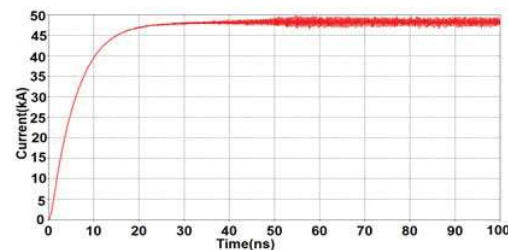


Fig. 10. Build-up of current with time

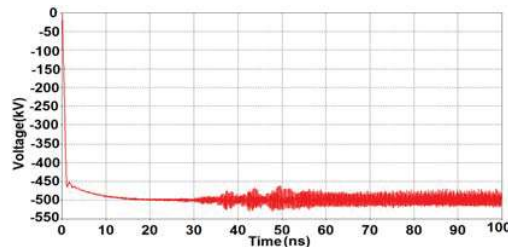


Fig. 11. Build-up of voltage with time

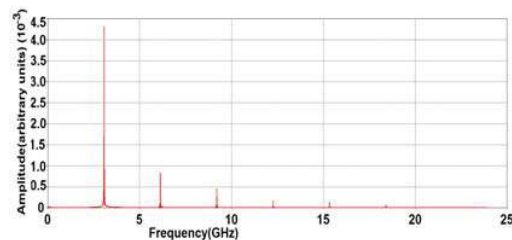


Fig. 12. Fourier transform of the electric field at the output port

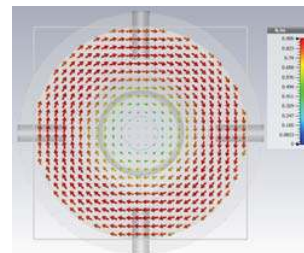


Fig. 13. The  $TM_{01}$  magnetic field distribution at the output port Schematic of coaxial disk loaded SWS



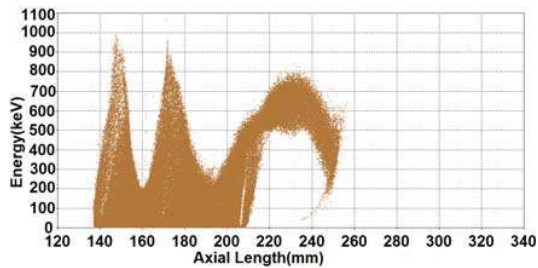


Fig. 14. Energy distribution against interaction length at 95 ns

## V. CONCLUSION

An improved S-band MILO has been designed using analytical method, and optimized and simulated using 3-D electromagnetic PIC code. The total length of the MILO has been significantly reduced by  $\sim 22\%$  as compared to the earlier conventional ones. A set of design parameters have been optimized for enhancement of conversion efficiency that includes reduction in length of cathode and beam dump, inner radii of choke and SWS vane, and placement of stubs. Reducing the length of cathode could manifest several advantages: (i) additional electrons are available for interaction with the desired operating mode for enhanced efficiency (ie. higher number of spoke electrons could participate in interaction), (ii) sufficient self-generation of magnetic field, and (iii) the reduced cathode length prevents cantilever axial shift and off-axis asymmetric emission of electron beam. The peak power of 6 GW and a frequency of 3.1 GHz at  $TM_{01}$ -mode with power conversion efficiency of  $\sim 25\%$  has been achieved with the diode voltage of 500 kV and current of 47.5kA.

## APPENDIX-A: VALIDATION

In order to validate the efficacy of the present analysis using CST Particle Studio, validation exercise has been carried out against a model of the device for which the details are available in the literature [16].

A comparison of the results are tabulated as shown in Table A.1. Typical simulated peak

output power and Fourier Transform of the electric field at the output port of MILO [16] are shown in Figs.A.1 and A.2 respectively.

Table A.1: Comparison of Results for Validation

Parameters	Results	
	Simulation using MAGIC [16]	Simulation using CST Particle studio
Beam Voltage	500 kV	500 kV
Beam Power	23.5 GW	23.5GW
Frequency	2.44 GHz	2.48GHz
RF Output Power	2.5 GW	2.54 GW
Power Conversion Efficiency	10.6 %	10.8 %

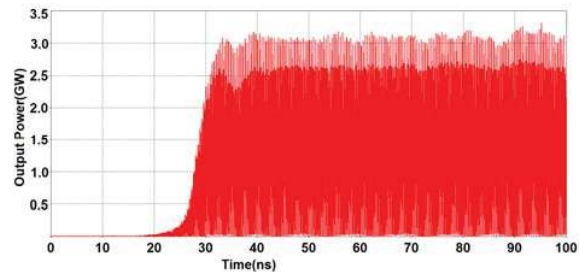


Fig. A.1 Peak output power of the MILO [16] obtained through CST simulation

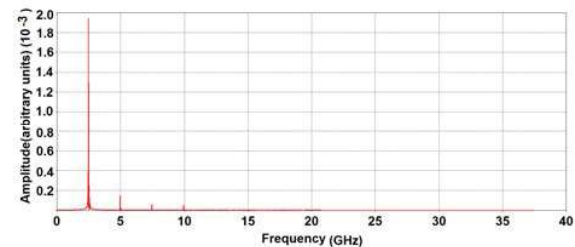


Fig. A.2 Fourier transform of the electric field at the output port of the MILO [16] obtained through CST simulation

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# **Electromagnetic Simulation and Experimental Characterization of RF Interaction Structure of an S-Band Magnetically Insulated Line Oscillator**

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**Abstract:** An S-band RF interaction structure of a Magnetically Insulated Line Oscillator (MILO) operating at fundamental-mode was designed using analytical formulations, and simulated using 3-D electromagnetic code CST Microwave Studio for its dispersion characteristics and RF output performance. The slow-wave structure was fabricated using precision CNC machining and characterized for its dispersion characteristics. The measured value of pi-mode frequency was found to be in close agreement (2.6%) with that from the simulation.

**Index Terms-** Dispersion relation, Coaxial disc-loaded waveguide, Magnetically insulated line oscillator (MILO), Slow-wave structure.

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## I. INTRODUCTION

Magnetically Insulated Line Oscillator (MILO) invented by Lemke and Clark in 1987 [1] became a popular choice as a high-power microwave (HPM) source for military applications. Its unique magnetic self-insulating property enables the device to handle large output power of the order of tens to hundreds of GW at a modest applied voltage of several hundreds of kilovolts. Moreover, no requirement of externally applied DC magnetic field also facilitates compact and lightweight configuration of the device. A basic configuration of the MILO is shown in Fig. 1 comprising of three major subsystems: (i) Cathode, (ii) Slow-wave structure (SWS) as a part of anode, and (iii) Collector or beam dump. At high voltages, electrons are emitted from the cathode and the current carried by the body (anode) creates a sufficiently strong magnetic field such that these electrons cannot cross the interaction gap. The electrons drift axially in the crossed electric and self-generated magnetic fields. The slow-wave structure (SWS) facilitates the interaction between the axially drifting electrons (the region adjacent to the cathode) and the axially directed slow electromagnetic wave to generate microwaves. However, it suffers from the fundamental limitation of low RF conversion efficiency. This is due to the utilization of maximum load current for generating the self-magnetic field [1]-[2].

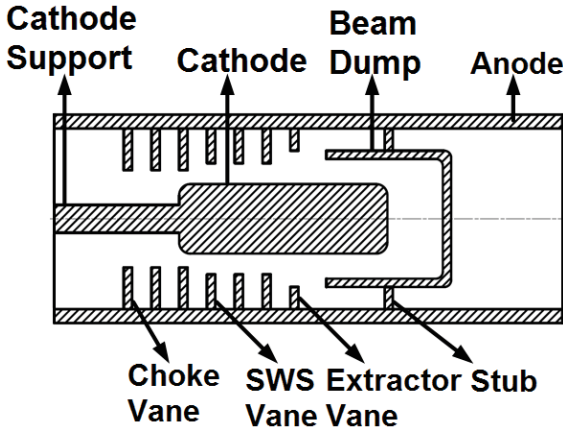


Fig.1. Schematic of Magnetically Insulated Line Oscillator

The first ever high-power MILO developed by Lemke *et al.* [3] could deliver output power of 2.1GW power at L-band having an efficiency of 10.3%. Cousin *et al.* developed a MILO with a 4-cavity slow-wave structure operating in  $3\pi/4$  mode at a beam voltage of 600 kV [4], for which the dispersion characteristics were obtained through simulation in 3D electromagnetic code MAGIC. In 2007, Dong Wang *et al.* [5] investigated the dispersion relation of coaxial disc-loaded SWS for symmetric and asymmetric modes using field matching approach. Yu-Wei Fan

*et al.* [6] used equivalent circuit analysis for obtaining the fundamental-mode frequency of MILO. Recently, Nallasamy *et al.*, [7] simulated an improved S-band MILO using CST Microwave Studio (efficiency enhanced to 25%) operating at the beam voltage of 500kV and current of 47.5kA.

Estimation of the fundamental frequency is a pre-requisite for designing the RF interaction structure (Fig. 2) of a MILO. For a cavity depth of  $d$ , the fundamental-mode frequency ( $f$ ) can be approximately estimated as  $f = c/4d$ , with  $c$  is the velocity of electromagnetic wave in free space. However, to the best of the knowledge of the present authors, there is no exact expression for accurate estimation of the fundamental-mode frequency other than field-analysis or 3D electromagnetic simulation. Field-analysis and/or 3D electromagnetic simulation invariably requires verification through cold-test measurements, as the analyses always have some approximations and assumptions.

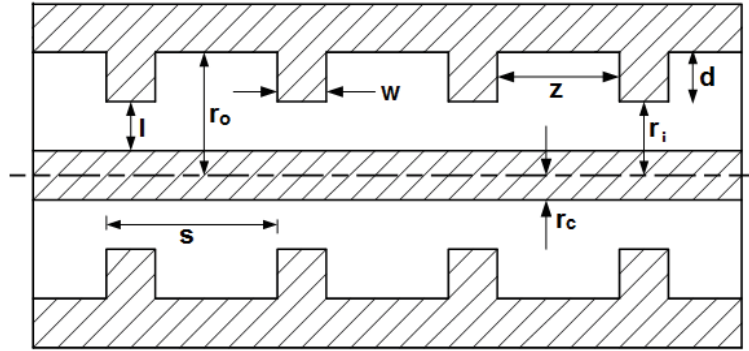


Fig. 2 Schematic of coaxial disc-loaded SWS.

In this paper, we present the design and simulation of the RF interaction structure of an S-band MILO. The design was carried out using analytical formulations and was simulated using 3D electromagnetic code CST Microwave Studio for obtaining the dispersion characteristics for the fundamental-mode operation. The RF interaction structure was fabricated with aluminum material and cold-test measurements were carried out for evaluating the dispersion characteristics. The paper is organized as follows: Design of the RF interaction structure is presented in Section-II and dispersion characteristics of the MILO by simulation and cold-test measurement are presented in Section III followed by the conclusion in Section IV.

## II. DESIGN OF RF INTERACTION STRUCTURE

We have considered a MILO with the slow-wave structure comprising periodically spaced cavities formed by placing concentric circular discs with apertures in a smooth waveguide, as shown in Fig. 2. The slow-wave structure supports number of slow-wave modes. Here,  $r_o$  and  $r_i$  are the outer and inner radii of the SWS vanes;  $d(=r_o - r_i)$  is the cavity depth;  $w$  is the

thickness of the SWS vane;  $z(=s-w)$  is the distance between the SWS apertures;  $r_c$  is the cathode radius;  $s$  is the circuit periodicity; and  $l = r_a - r_c$  is the free space gap between anode to cathode.

As the cathode current reaches beyond the critical current, the self-magnetic field generated therein confines the electrons and prevents them reaching upto the anode. The electrons derive equipotential surfaces and move perpendicular to the crossed electric and magnetic fields. The minimum current or critical current  $I_{cr}$  required to insulate the beam is defined as [8]:

$$I_{cr} = \frac{4\pi m_0 c^3 \varepsilon_0 \sqrt{\gamma_0^2 - 1}}{e \ln(r_a/r_c)} \quad (1)$$

$$= \frac{I_0 \sqrt{\gamma_0^2 - 1}}{2 \ln(r_a/r_c)}$$

where,  $I_0 = (4\pi m_0 c^3 \varepsilon_0) / e$  is the starting current for oscillation,  $e$  is the electron charge,  $m_0$  is the electron mass at rest, and  $\gamma_0 (= 1 + eV_0/m_0c^2)$  is the relativistic mass factor with  $V_0$  as the beam voltage. Under the condition of the insulated electron flow filling the anode-to-cathode gap, the total anode current or the para-potential current ( $I_p$ ) becomes [8]:

$$I_p = \frac{I_0 \gamma_0 \ln(\gamma_0 + \sqrt{\gamma_0^2 - 1})}{2 \ln(r_a/r_c)} \quad (2)$$

At the prevailing condition of Diocotron instability [9], some of the electrons of the beam reach the anode and some others remain at the magnetic cutoff, while the other electrons migrate towards the anode by forming bunches or spokes. The mode of oscillation of MILO is established when electron drift velocity is slightly greater than the phase velocity of the RF wave. The condition of synchronism is given as [10]:

$$v_d = \frac{E_0}{B_0} = \frac{V_0}{2 \ln(r_a/r_c)} \left( \frac{2\pi r}{\mu_0 I_t} \right) = \frac{2\pi \varepsilon_0 c^2}{\ln(r_a/r_c)} \left( \frac{V_0}{I_t} \right) \cong 0.3c \quad (3)$$

Here,  $v_d$  is the electron drift velocity,  $\varepsilon_0$  is the permittivity of free-space and  $I_t$  is the total anode current. The RF phase velocity ( $v_\phi$ ) at under the condition of synchronism ( $v_\phi \cong v_d$ ) can be expressed as [10]:

$$v_\phi = \frac{s}{2d/c} \cong 0.3c = \frac{\omega}{\beta_0} = \frac{2\pi f}{(\pi/s)} = 2sf \quad (4)$$

Here,  $\omega$  is the angular frequency and  $\beta_0$  is the axial propagation constant. At the beam voltage of 500kV and impedance of 25  $\Omega$ , the ratio of the inner radius of the anode to the cathode radius is given by [10]:

$$\frac{r_i}{r_c} = 1.6 \quad (5)$$

The design starts with the inputs: the operating frequency ( $f$ ), beam voltage ( $V_0$ ), cathode radius ( $r_c$ ) and the width of the SWS vane ( $w$ ) is chosen with practical considerations [3], [7], [10]. The values of the circuit periodicity ( $s$ ) and cavity depth ( $d$ ), are arrived at using the condition of synchronism ( $v_\phi \cong v_d$ ) and the expressions (3) and (4) with the known value of operating frequency ( $f$ ). The expressions (1) and (2) are used with the known value of beam voltage ( $V_0$ ) and ( $r_i/r_c$ ) from (5) to arrive at the critical current for self-magnetic insulation and total current in the device for sustainable oscillation. The value of inner radius of the SWS vane ( $r_i$ ) is directly calculated using (5); and the value of outer radius of the SWS ( $r_0$ ), interaction gap ( $z$ ) and the free space gap between anode to cathode ( $l$ ) are obtained from the relations,  $r_0 = r_i + d$ ,  $z = s - w$  and  $l = r_i - r_c$ , respectively. The dimensions of the slow-wave structure thus arrived at are:  $r_c = 25$  mm;  $r_i = 40$  mm;  $r_0 = 61.4$  mm;  $s = 13$  mm;  $d = 21.4$  mm;  $w = 4$  mm;  $z = 9$  mm; and  $l = 15$  mm.

### III. SIMULATION AND COLD-TEST MEASUREMENT

The present RF interaction structure consists of 4 cavities (3 full cavities and 2 half cavities) along with two co-axial probes of 50 $\Omega$  impedance with SMA-type connectors. The structure has been modeled along with the cathode with one probe as the input port and the other probe as the output port. The 3D modeling of the device was carried out using CST Studio with adaptive mesh refinement. The 3D model of the RF interaction structure with short-length cathode and probes is shown in Fig.3. SWS vanes, cathode, anode, and probes of MILO structure have been modeled using a perfect electric conductor (PEC) with background as vacuum. The MILO structure has been modeled and simulated in the linear co-ordinate system with hexahedral meshing using the time domain solver module of CST microwave studio. The time domain analysis confirms the  $\pi$ -mode of operation at 3.7 GHz. The return loss versus frequency and the dispersion characteristics as obtained from the simulation are shown in Fig. 4 and Fig. 5, respectively.



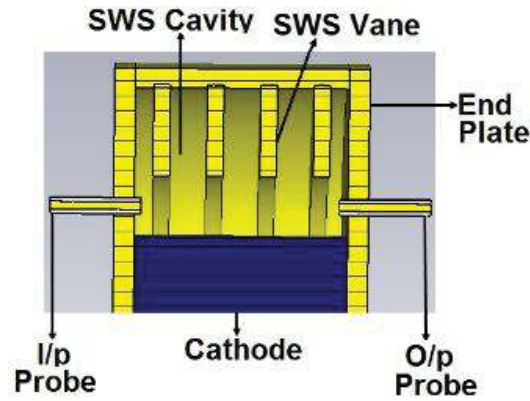


Fig. 3 Cut view of the RF interaction structure along with the cathode and the coupling probes

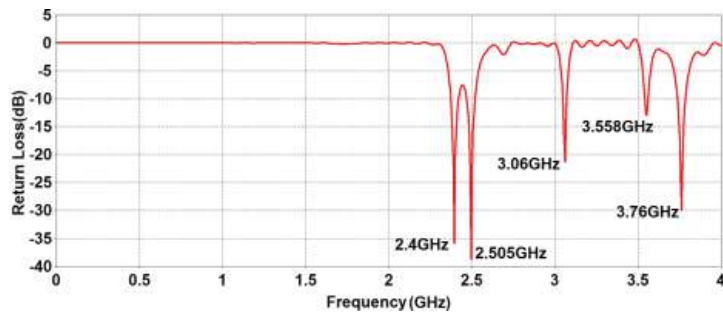


Fig. 4  $S_{11}$  plot of the RF interaction structure against frequency

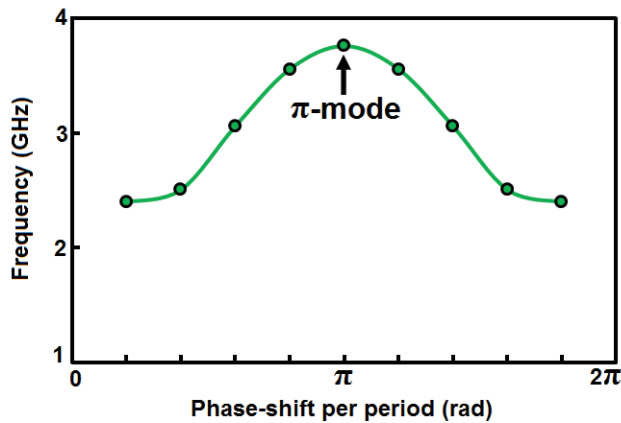


Fig. 5 Dispersion characteristics of the RF interaction structure

Subsequent to the design and simulation, the RF interaction structure was developed with SMA-type input and output couplers. RF signal (0 dBm) was fed from a Network Analyzer to the cavity with the other port of the cavity terminated to a matched load as shown in Fig. 6. The return loss profile of the structure as obtained in the Network Analyzer is shown in Fig. 8.

It may be noted from the cold test measurement that 5 resonant frequencies are observed in the return loss profile: 2.4 GHz, 2.505 GHz, 3.06 GHz, 3.558 GHz, and 3.76 GHz. These frequencies are interpreted to obtain the dispersion characteristics as compared against simulation in Fig. 9. The measured pi-mode frequency was found to be 3.86 GHz against the simulated value of 3.76 GHz (deviation of around 2.6% with regard to simulation). The shift in simulated  $\pi$ -mode frequency from the design frequency of 3.3 GHz is due to the insertion of probes on both sides of the RF interaction structure caused the perturbation of electric field inside the RF interaction structure. The deviation in measured  $\pi$ -mode frequency is mainly due to the fabrication tolerances and the corner radius in the experimental cavity along with perturbation of electric field caused by the insertion of probes on both sides of the RF interaction structure.



Fig. 6 Fabricated RF interaction structure



Fig. 7 Components of the RF interaction structure

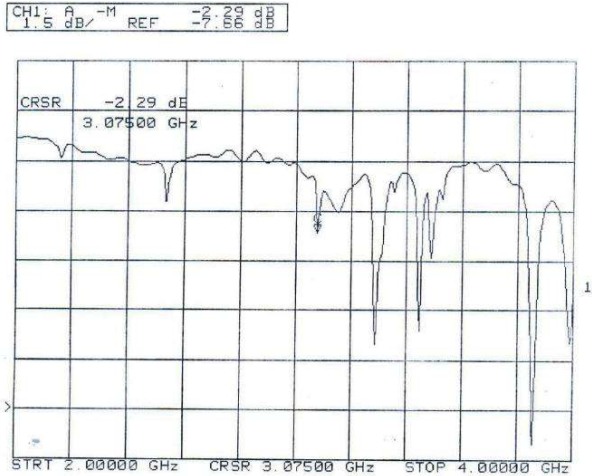


Fig. 8 Measured  $S_{11}$  performance of the RF interaction structure

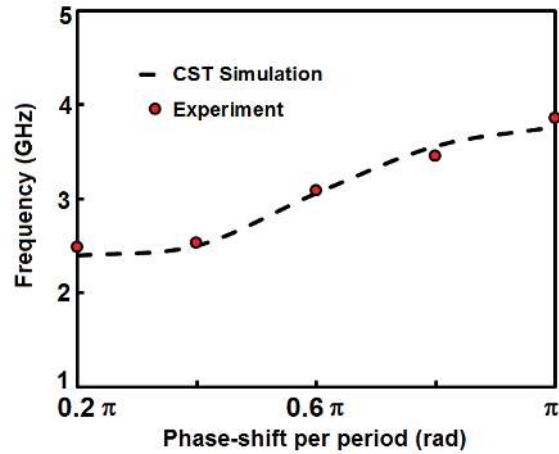


Fig. 9 Comparison of simulation and cold-test measurement

#### IV. CONCLUSION

The RF interaction structure of an experimental S-band MILO, with single-shot output power of around 2.5 GW, has been designed and the beam absent (cold) electromagnetic simulation, has been carried out using CST Microwave Studio by inserting probes on both sides of RF interaction structure. Based on the design and cold simulation, the assembly and piece parts have been fabricated and assembled for cold test measurements using scalar network analyzer (SNA) based on resonant perturbation method. Comparing with the design  $\pi$ -mode frequency of 3.3 GHz, the change in cold simulated  $\pi$ -mode frequency is due to the perturbation of electric field by the insertion of probes on both sides of the RF interaction structure. The deviation in measured  $\pi$ -mode frequency against the design and simulated  $\pi$ -mode frequency is mainly due to the fabrication tolerances along with perturbation of electric field caused by the insertion of probes. The measured results are validated against the simulated results of design  $\pi$ -mode frequency. The results obtained from both simulation and measurement are in close agreement, showing the efficacy of the design.

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